

Compact Ultra-Wideband Bandpass Filters Using Composite Microstrip–Coplanar-Waveguide Structure

Tsung-Nan Kuo, Shih-Cheng Lin, and Chun Hsiung Chen, *Fellow, IEEE*

Abstract—Compact ultra-wideband bandpass filters are proposed based on the composite microstrip–coplanar-waveguide (CPW) structure. In this study, the microstrip–CPW transitions and the CPW shorted stubs are adopted as quasi-lumped-circuit elements for realizing a three-pole high-pass filter prototype. By introducing a cross-coupled capacitance between input and output ports of this high-pass filter and suitably designing the transition stretch stubs, a compact three-pole ultra-wideband bandpass filter is implemented with two transmission zeros located close to the passband edges. To further improve the selectivity, two microstrip shorted stubs are added to implement a five-pole ultra-wideband bandpass filter with good out-of-band response. Being developed from the quasi-lumped elements, and not from the transmission lines, the proposed ultra-wideband filters have sizes more compact than those of the published wideband filters. The proposed ultra-wideband filters have the merits of compact size, flat group delay, good insertion/return loss, and good selectivity. Agreement between simulated and measured responses of these filters is demonstrated.

Index Terms—Bandpass filter, coplanar waveguide (CPW), cross coupling, high-pass filter, microstrip, ultra-wideband (UWB).

I. INTRODUCTION

ULTRA-WIDEBAND (UWB) radio technology has been getting more and more popular for high-speed wireless connectivity, since the Federal Communications Commission (FCC)'s decision to permit the unlicensed operation band from 3.1 to 10.6 GHz in February 2002 [1]. There are several advantages for UWB radio system, such as transmitting higher data rates, needing lower transmit power, and simplifying the error control coding. In such a system, an UWB filter is one of the key components, which should exhibit a wide bandwidth with low insertion loss over the whole band. In order to meet the FCC limit, good selectivity at both lower and higher frequency ends and flat group-delay response over the whole band are required.

The conventional filter synthesis procedure is adequate only for the relatively narrowband filters, and is not suitable for the wideband filters [2]. Basically, a wide bandwidth filter may be implemented by a direct cascade of the low- and high-pass filters. In [3], the wideband coplanar-waveguide (CPW) bandpass filters based on the cascade of CPW low- and high-pass periodic structures were constructed. To save the circuit area, the

wideband bandpass filters were proposed by combining the low- and high-pass filters together [4]. These wideband filters have good suppression on out-of-band response, however, they have the drawback of large circuit size or imperfect group delay over the passband.

To meet the UWB filter specification, several studies to increase the number of sections have been reported. In [5], the high-pass filter consisting of a cascade of shunt short-circuited stubs was adopted for the UWB filter design. In [6], the UWB filter was constructed by a cascade of various ring filters. These UWB filters have sharp rejection, but their spurious response would degrade the out-of-band response and an increase in number of sections may lead to large insertion loss, as well as poor group delay.

Another way to realize wideband bandpass filters is to use the parallel-coupled lines [7], [8]. In [9], the parallel-coupled microstrip line with defected ground was employed to give a tight coupling for a wideband bandpass filter. However, the more the fractional bandwidth is required, the smaller the gap size is demanded to enhance the coupling. In [10], by adding a third line in the parallel coupled line design, the restriction on gap size may be relaxed for a specific coupling, but for UWB filter design, the necessary gap size is still too narrow to be fabricated.

Recently, broadside-coupled structures have received great attention due to the merit associated with the electromagnetic coupling. The CPW-to-CPW transitions were first proposed in [11], accompanied by the development of CPW-to-microstrip transitions [12] and microstrip-to-CPW transitions [13]. In [14], the UWB filter with a multiple-mode resonator was proposed using the microstrip-to-CPW transitions as inverter circuits. Recently, a UWB filter was proposed using the microstrip-to-CPW transitions to realize the broadside-coupled structure and then cascading three sections to give good selectivity [15].

In this paper, compact UWB bandpass filters are developed by adopting the high-pass filter prototype and transition stretch stubs to create the lower and upper stopbands, respectively. Specifically, a composite microstrip–CPW structure is proposed to realize a lumped-element high-pass filter prototype, which is essential in developing the UWB bandpass filters. First, by using the microstrip-to-CPW transition structures to implement two series lumped capacitors, using a CPW shorted stub structure to implement the shunt inductor, and also introducing a suitable cross-coupled capacitor between the input and output ports, a very wideband three-pole bandpass filter is developed from the corresponding three-pole high-pass filter prototype. Second, by suitably modifying the shape of

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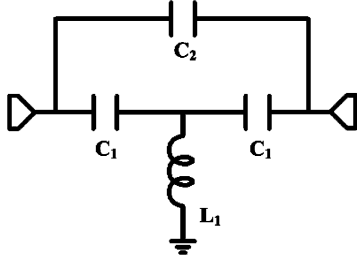


Fig. 1. Circuit diagram of the three-pole high-pass filter prototype.

microstrip-to-CPW transition to create the microstrip stretch stub for adjusting the upper transmission zero, a three-pole UWB bandpass filter is fabricated with two transmission zeros properly located. Finally, to give more sharp rejection around the upper stopband, two microstrip shorted stubs are incorporated into the three-pole UWB bandpass filter so that a five-pole UWB bandpass filter is implemented. Being that the quasi-lumped elements in the filter design is adopted, the proposed UWB filters exhibit the slow wave behavior and have sizes more compact than those of published wideband filters.

II. HIGH-PASS-BASED BANDPASS FILTER

Fig. 1 shows the lumped-element three-pole high-pass filter prototype that will be adopted to develop a very wideband bandpass filter. Here, the series capacitances C_1 and shunt inductance L_1 are selected to decide the cutoff frequency of the high-pass filter, and the cross-coupled capacitance C_2 is introduced to create a transmission zero at the passband edge so that the filter selectivity at the lower stopband may be improved. Fig. 2(a) shows the circuit simulated frequency response of this three-pole high-pass filter prototype for which the value of cross-coupled capacitance C_2 is adjusted to control the location of the created transmission zero.

The even- and odd-mode analysis technique can be used to discuss the transmission zero [16]. By symmetry of the circuit model in Fig. 1, the even- and odd-mode input impedances (Z_{even} and Z_{odd}) are expressed as

$$Z_{\text{even}} = j \left(2wL_1 - \frac{1}{wC_1} \right) \quad (1)$$

$$Z_{\text{odd}} = \frac{1}{jw(C_1 + 2C_2)}. \quad (2)$$

By superposition, the transfer function S_{21} is written as

$$S_{21} = \frac{(Z_{\text{even}} - Z_{\text{odd}})Z_0}{(Z_{\text{even}} + Z_0)(Z_{\text{odd}} + Z_0)} \quad (3)$$

where Z_0 is the impedance of the input port. A transmission zero is created when the transfer function S_{21} is equal to zero, i.e.,

$$Z_{\text{even}} = Z_{\text{odd}}. \quad (4)$$

By using (4), the location of transmission zero may be predicted. Fig. 2(b) shows the curve to relate the transmission-zero fre-

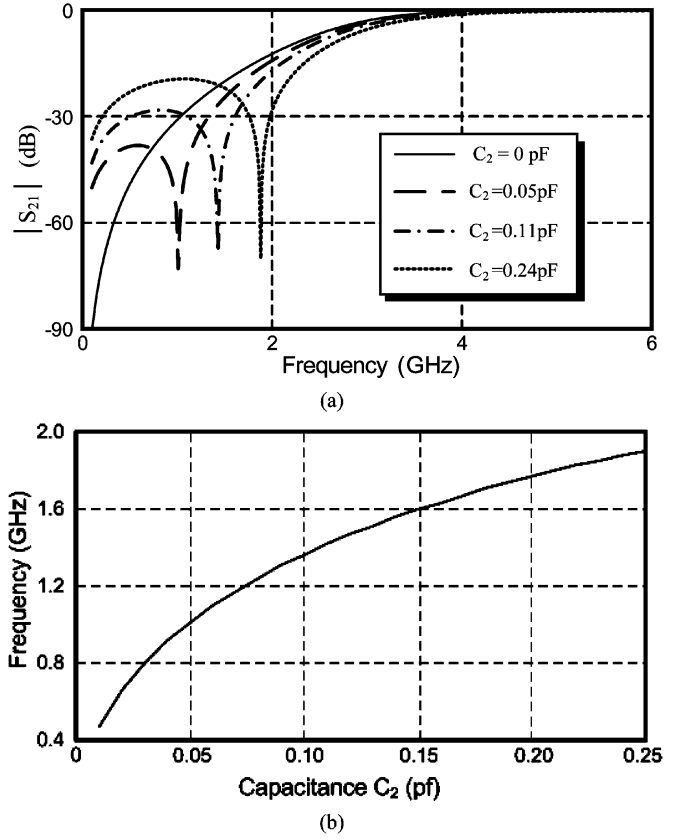
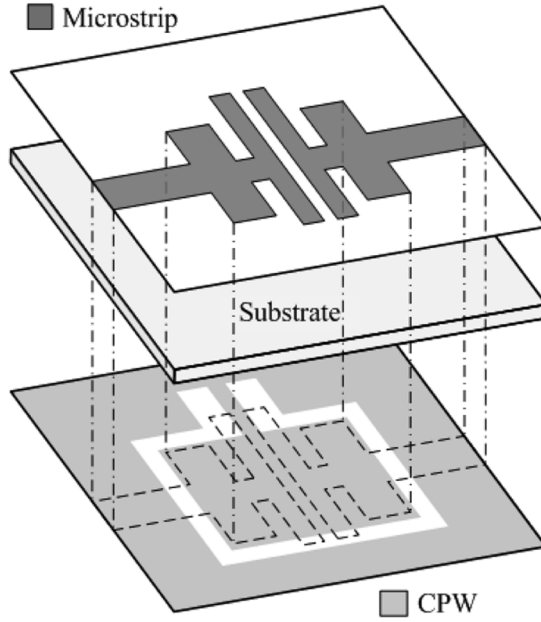


Fig. 2. (a) Circuit simulated results of the three-pole high-pass filter prototype (Fig. 1) for various values of the cross-coupled capacitance C_2 . (b) Curve to relate the transmission-zero frequency to the value of the capacitance C_2 . ($C_1 = 0.858$ pF, $L_1 = 1.5$ nH).

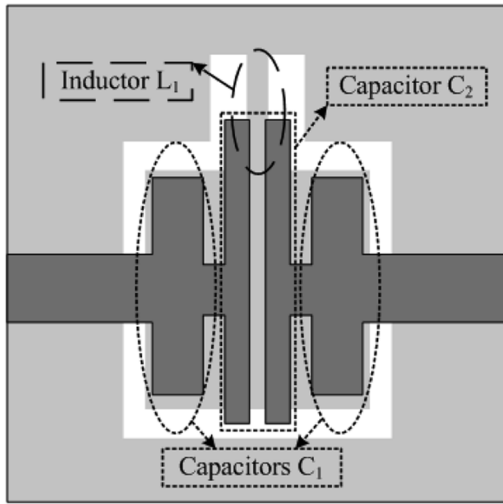
quency to the value of cross-coupled capacitance C_2 under the case of $C_1 = 0.858$ pF and $L_1 = 1.5$ nH. As the value of C_2 increases, the transmission zero will move toward the higher frequency.

To realize the circuit model in Fig. 1, the series capacitors C_1 are implemented by the microstrip-to-CPW transitions, and the shunt inductor L_1 is implemented by the CPW shorted stub connected to the ground. The cross-coupled capacitor C_2 is formed between the adjacent microstrip parts of the two capacitors C_1 . Fig. 3(a) and (b) shows the three-dimensional and top-/bottom-layer circuit layouts of the proposed filter, respectively, which is developed from the high-pass filter prototype shown in Fig. 1.

The full-wave simulated results of Fig. 3 are shown in Fig. 4, which are calculated by the ADS Momentum simulator and simulated on the substrate with $\epsilon_r = 3.38$, $\tan \delta = 0.002$, and thickness $h = 0.508$ mm. Although the circuit layout (Fig. 3) is developed from the high-pass filter prototype (Fig. 1), the implemented structure (Fig. 3) actually behaves like a wideband bandpass filter for which a stopband starts to appear at 17 GHz. Basically, this implemented filter has a very wideband with a 3-dB fractional bandwidth of 134% from 3.07 to 15.7 GHz and two transmission zeros are found at 1.88 and 16.81 GHz. Note that the first transmission zero is created by the cross-coupled capacitance C_2 and the second transmission zero is generated by the resonance associated with the microstrip parts of the capacitors C_2 and the CPW shorted stub. The filter has a min-



(a)



(b)

Fig. 3. (a) Three-dimensional circuit layout of proposed wideband filter. (b) Top-/bottom-layer circuit layouts to show the relative location between top microstrip and bottom CPW layers of proposed wideband filter.

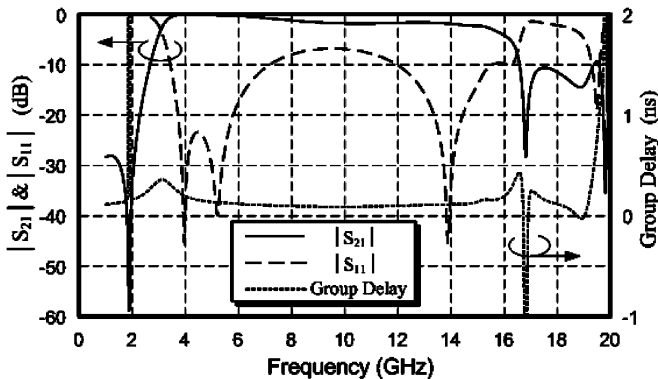


Fig. 4. Simulated results of the proposed filter in Fig. 3.

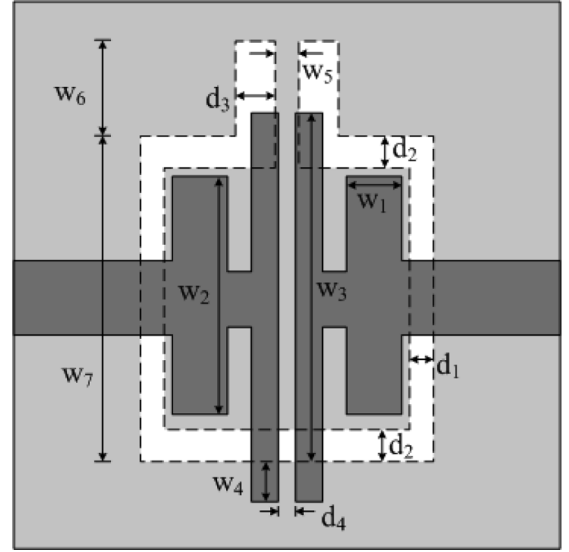


Fig. 5. Top-/bottom-layer circuit layouts of proposed three-pole UWB bandpass filter. ($w_1 = 0.89$ mm, $w_2 = 3.81$ mm, $w_3 = 5.59$ mm, $w_4 = 0.635$ mm, $w_5 = 0.38$ mm, $w_6 = 1.52$ mm, $w_7 = 5.21$ mm, $d_1 = 0.38$ mm, $d_2 = 0.5$ mm, $d_3 = 0.635$ mm, and $d_4 = 0.28$ mm).

imum insertion loss of 0.1 dB, and the return loss is greater than 6.8 dB within the passband. Moreover, this filter has a compact dimension of $4.7 \text{ mm} \times 6.73 \text{ mm}$, which is approximately $0.243 \lambda \times 0.347 \lambda$, and λ is the guided wavelength of the microstrip structure at the center frequency $f_0 = 9.32$ GHz. In addition, this wideband bandpass filter exhibits a flat group-delay response below 0.35 ns over the whole passband.

III. THREE-POLE UWB BANDPASS FILTER

In Section II, a very wideband bandpass filter is constructed from the three-pole high-pass filter prototype. In order to develop a filter meeting the UWB standard, the high-frequency response needs to decay early. To this end, the microstrip-to-CPW transition structure in Fig. 3 is modified such that part of the microstrip segment is extended over the ground region of microstrip to form a transition stretch stub of length w_4 , as shown in Fig. 5. By this modification, a three-pole UWB bandpass filter (shown in Fig. 5) is developed.

For the proposed three-pole UWB bandpass filter with the circuit layout shown in Fig. 5, the microstrip-to-CPW transitions are used to realize the series capacitances C_1 and the CPW shorted stub connected to ground is used to realize the shunt inductance L_1 . The adjacent microstrip parts between two transitions are used to implement the cross-coupled capacitance C_2 . Note that the adjacent microstrip portions of two transitions have parts of microstrip segments, the transition stretch stubs, extending over the ground. These stretch stubs are used to generate the transmission zero at the upper passband edge so that the selectivity of the UWB bandpass filter around the upper stopband may be improved.

Fig. 6(a) illustrates the effect of adjusting the length w_4 of the transition stretch stub covering the ground. It shows that an additional transmission zero will be observed at the higher frequency. Specifically, the upper transmission zero will move to

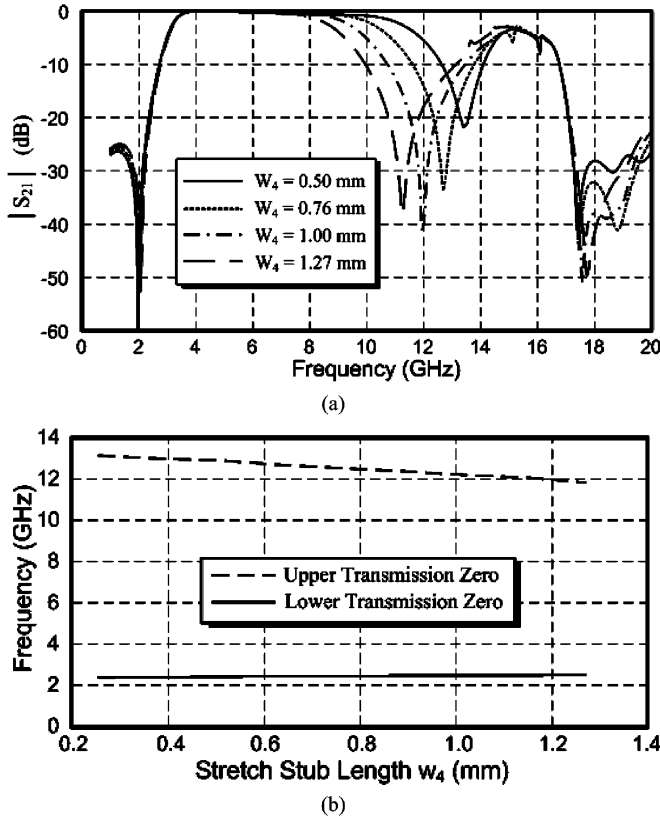


Fig. 6. (a) Simulated results of the proposed three-pole UWB filter (Fig. 5) for various values of the stretch stub length w_4 . (b) Curves to relate the transmission-zero frequencies to the values of the stretch stub length w_4 .

the lower frequency as the stretch stub length w_4 is increased. Note that an adjustment of the stretch stub length w_4 also has a minor effect on the cross-coupled capacitance C_2 with the lower transmission zero moving slightly to the high frequency as w_4 is increased. The transmission-zero frequency versus the stretch stub length w_4 is plotted in Fig. 6(b), where the upper transmission zero decreases almost linearly and the lower transmission zero increases slightly when the length w_4 is increased. By designing a three-pole high-pass filter and introducing a suitable stretch stub, a compact three-pole UWB bandpass filter is implemented with two transmission zeros located close to the pass-band edges.

Fig. 7(a) shows the measured and full-wave simulated responses of the three-pole UWB bandpass filter (Fig. 5), which is fabricated on the Rogers RO4003C substrate with $\epsilon_r = 3.38$, $\tan \delta = 0.002$, and thickness $h = 0.508$ mm. The measured center frequency is at 6.8 GHz and the measured 3-dB fractional bandwidth is 109.7% from 3.07 to 10.53 GHz. This implemented filter has a minimum insertion loss of 0.4 dB, and the return loss is greater than 11 dB within the passband. Two transmission zeros are found at 1.919 and 13.07 GHz. The implemented filter with the input and output feeding transmission lines deembedded presents a flat group-delay response below 0.36 ns over the whole passband. Note that the group delay exhibits negative numbers around the frequencies at which the transmission zeros are observed, as shown in Fig. 7(b). Besides, the proposed three-pole UWB bandpass filter has a very

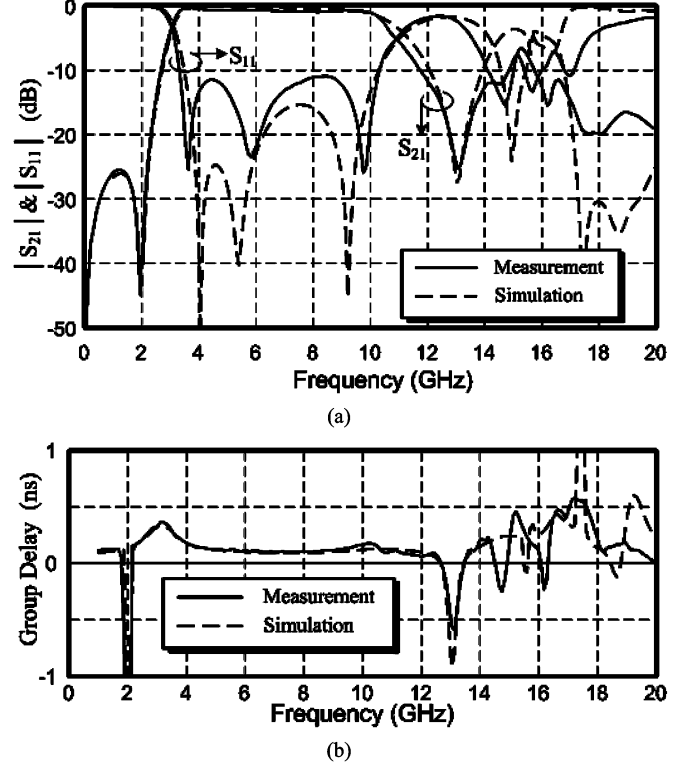


Fig. 7. Measured and simulated results of the proposed three-pole UWB filter (Fig. 5). (a) Scattering parameters. (b) Group delay.

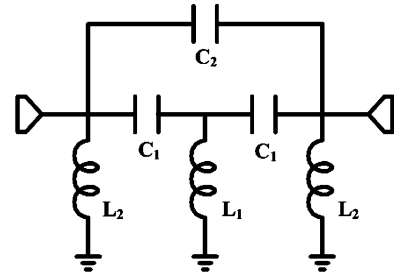


Fig. 8. Circuit diagram of the five-pole high-pass filter prototype.

compact size of $4.7 \text{ mm} \times 6.73 \text{ mm}$, which is approximately $0.177 \lambda \times 0.253 \lambda$ and where λ is the guided wavelength of microstrip structure at the center frequency $f_0 = 6.8$ GHz.

IV. FIVE-POLE UWB BANDPASS FILTER

Although the three-pole UWB bandpass filter (Fig. 5) shows good performance and compact size, it still cannot meet the FCC's limit due to its poor selectivity at higher frequency. To improve the selectivity and to have more attenuation in the stopband, one may modify the three-pole UWB bandpass filter structure in Fig. 5 to form a new five-pole UWB bandpass filter, which is also developed from a five-pole high-pass filter prototype.

Shown in Fig. 8 is the circuit model of a five-pole high-pass filter prototype, as discussed in [2]. By inserting a cross-coupled capacitance C_2 between the input and output ports of the five-pole high-pass filter prototype, a transmission zero can be created at the lower stopband, as shown in Fig. 9(a). Due to the

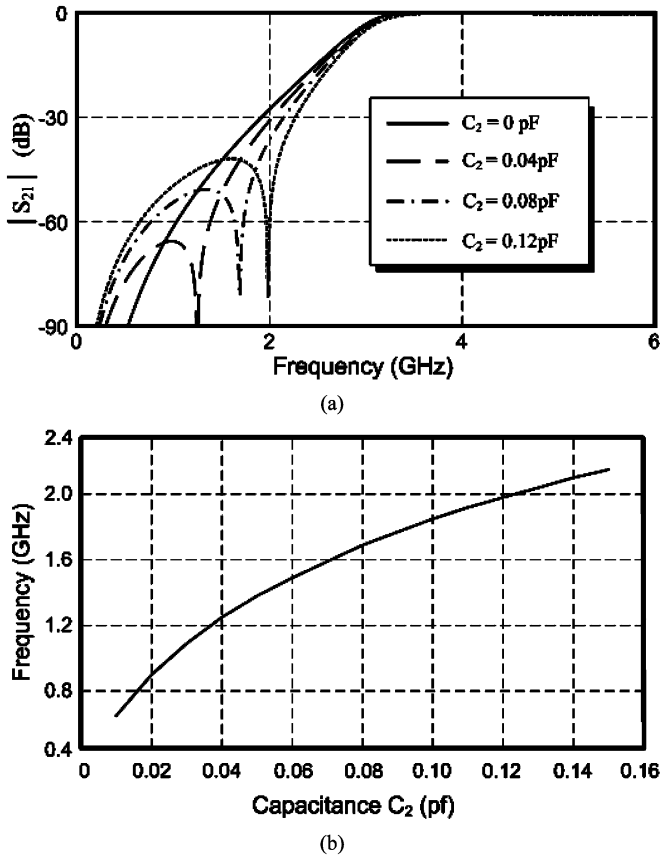


Fig. 9. (a) Circuit simulated results of the five-pole high-pass filter prototype (Fig. 8) for various values of the cross-coupled capacitance C_2 . (b) Curve to relate the transmission-zero frequency to the value of the capacitance C_2 . ($L_1 = 1$ nH, $C_1 = 0.768$ pF, $L_2 = 1.8$ nH).

symmetry of the circuit diagram (see Fig. 8), the transmission zero may also be discussed by the even- and odd-mode analysis technique. For the case of $L_1 = 1$ nH, $C_1 = 0.768$ pF, and $L_2 = 1.8$ nH, the curve to relate the transmission-zero frequency to the value of the cross-coupled capacitance C_2 is plotted in Fig. 9(b). Note that the transmission zero will move toward the higher frequency as the value of C_2 increases.

Fig. 10 shows the circuit layout of the proposed five-pole UWB bandpass filter. This implemented filter is based on the five-pole high-pass filter prototype in Fig. 8. Again, the series capacitors C_1 are implemented by the microstrip-to-CPW transitions and the shunt inductor L_1 is implemented by a CPW shorted stub connected to the ground. The cross-coupled capacitance C_2 is realized by the adjacent microstrip parts of the two capacitors C_1 . The shunt inductors L_2 are implemented by the microstrip shorted stubs with metal vias to the ground and the metal via has a diameter of 1 mm. Note that an adjustment of the stretch stub length w_4 is essential in controlling the transmission-zero frequency near the upper passband edge.

As shown in Fig. 11(a), an additional upper transmission zero would be observed at the higher frequency. When the stretch stub length w_4 increases, the upper transmission zero would move to the lower frequency, accompanied by a slight increase of cross-coupled capacitance C_2 to make the lower transmission zero slightly move to the high frequency. The curves to depict

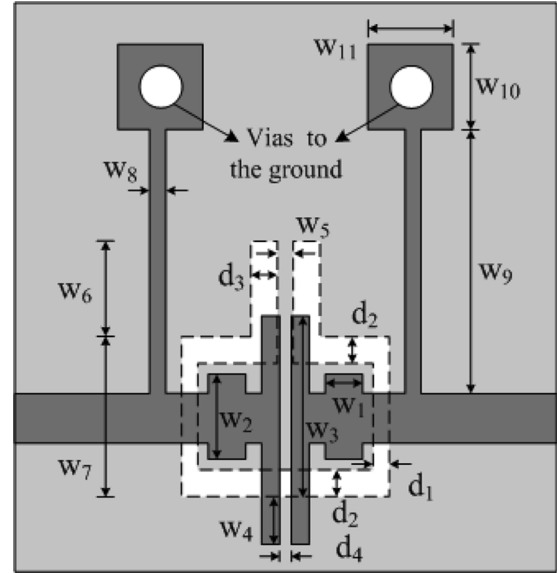


Fig. 10. Top-/bottom-layer circuit layouts of proposed five-pole UWB band-pass filter. ($w_1 = 0.89$ mm, $w_2 = 2.03$ mm, $w_3 = 4.318$ mm, $w_4 = 1.143$ mm, $w_5 = 0.38$ mm, $w_6 = 2.29$ mm, $w_7 = 3.81$ mm, $w_8 = 0.38$ mm, $w_9 = 6.22$ mm, $w_{10} = 2.03$ mm, $w_{11} = 2.03$ mm, $d_1 = 0.38$ mm, $d_2 = 0.635$ mm, $d_3 = 0.635$ mm, and $d_4 = 0.28$ mm).

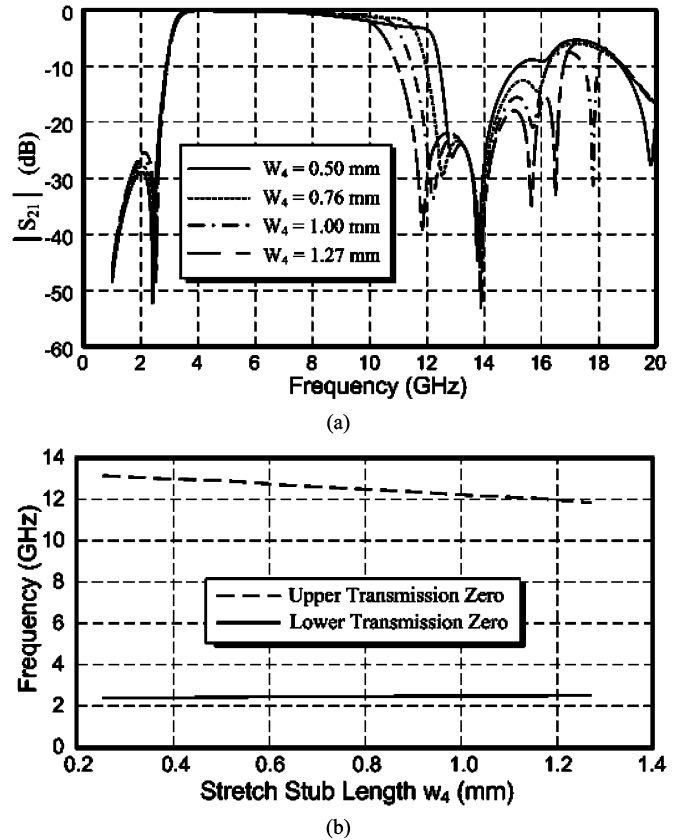


Fig. 11. (a) Simulated results of the proposed five-pole UWB filter (Fig. 10) for various values of the stretch stub length w_4 . (b) Curves to relate the transmission-zero frequencies to the values of the stretch stub length w_4 .

the relation between two transmission zeros and the stretch stub length w_4 are shown in Fig. 11(b), where the upper transmission zero decreases almost linearly and the lower transmission

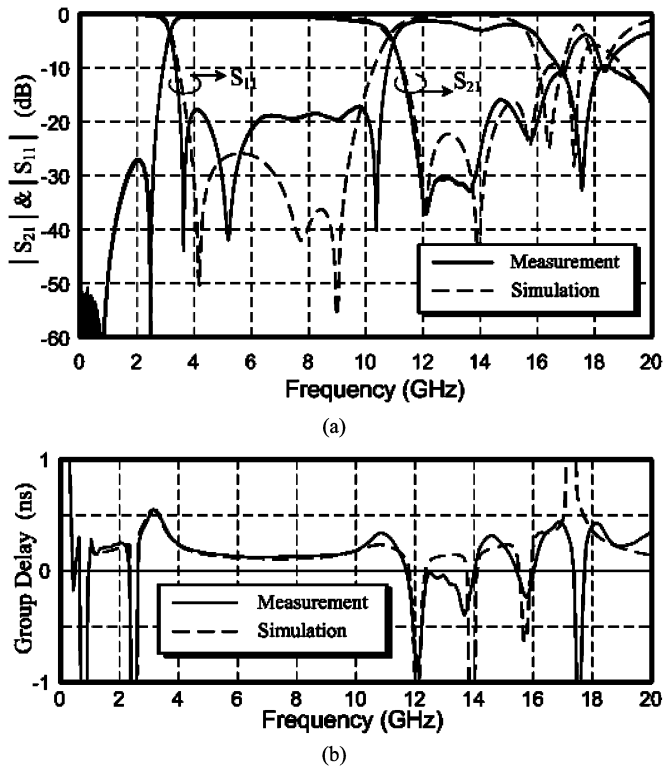


Fig. 12. Measured and simulated results of the proposed five-pole UWB filter (Fig. 10). (a) Scattering parameters. (b) Group delay.

zero increases slightly with the increasing stretch stub length w_4 . After suitably designing the transition stretch stubs to the filter (Fig. 10), a five-pole UWB bandpass filter is proposed.

The measured and full-wave simulated responses of the five-pole UWB bandpass filter (Fig. 10) are shown in Fig. 12(a) with the filter again fabricated on the Rogers RO4003C substrate. The measured center frequency is at 6.95 GHz and the measured 3-dB fractional bandwidth is 108.5% from 3.18 to 10.72 GHz. This implemented filter has a minimum loss of 0.48 dB, and the return loss is greater than 17.2 dB within the passband. Three transmission zeros are found at 2.45, 12.11, and 13.63 GHz. The first and second transmission zeros are generated by the cross-coupled capacitance and stretch stubs, respectively. Note that the third transmission zero is produced due to the resonance of the microstrip shorted stubs. With these transmission zeros, the five-order UWB bandpass filter has good selectivity and stopband rejection. Moreover, the implemented filter with the feeding lines deembedded exhibits flat group-delay response below 0.55 ns over the whole passband, as shown in Fig. 12(b). As in the case of the three-pole UWB bandpass filter, the group delay also exhibits the negative numbers around the frequencies of the transmission zeros. Besides, the proposed five-pole UWB bandpass filter has a very compact size of $8 \text{ mm} \times 11.9 \text{ mm}$, which is approximately $0.306 \lambda \times 0.458 \lambda$ at the center frequency ($= 6.95 \text{ GHz}$).

V. CONCLUSION

In this paper, three- and five-pole UWB bandpass filters based on the microstrip-to-CPW transitions and CPW/microstrip

shorted stubs connected to the ground have been implemented and carefully examined. By introducing a cross-coupled capacitance to the high-pass filter prototype and suitably designing the transition stretch stubs, the lower and upper transmission zeros have been generated and properly located. In the five-pole UWB bandpass filter, two microstrip shorted stubs used to realize two shunt inductances would resonate at higher frequency, thereby producing the third transmission zero at this higher frequency. With these transmission zeros, the proposed filters have good selectivity and stopband rejection. In addition, the dimensions of proposed UWB bandpass filters are much less than those of the published UWB filters. The proposed filters with good frequency performance and flat group delay are attractive for UWB radio applications.

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REFERENCES

- [1] "Revision of part 15 of the Commission's rules regarding ultra-wideband transmission systems," FCC, Washington, DC, Tech. Rep. ET-Docket 98-153, FCC02-48, adopted in Feb. 2002.
- [2] J. S. Hong and M. J. Lancaster, *Microstrip Bandpass Filters for RF/Microwave Applications*. New York: Wiley, 2001.
- [3] Y. S. Lin, W. C. Ku, C. H. Wang, and C. H. Chen, "Wideband coplanar-waveguide bandpass filters with good stopband rejection," *IEEE Microw. Wireless Compon. Lett.*, vol. 14, no. 9, pp. 422–424, Sep. 2004.
- [4] C. L. Hsu, F. C. Hsu, and J. T. Kuo, "Microstrip bandpass filter for ultra-wideband (UWB) wireless communications," in *IEEE MTT-S Int. Microw. Symp. Dig.*, 2005, pp. 679–682.
- [5] W. T. Wong, Y. S. Lin, C. H. Wang, and C. H. Chen, "Highly selective microstrip bandpass filters for ultra-wideband (UWB) applications," in *Proc. Asia-Pacific Microw. Conf.*, Nov. 2005, pp. 2850–2853.
- [6] H. Ishida and K. Araki, "Design and analysis of UWB bandpass filter with ring filter," in *IEEE MTT-S Int. Microw. Symp. Dig.*, Jun. 2004, pp. 1307–1310.
- [7] W. Menzel, L. Zhu, K. Wu, and F. Bogelsack, "On the design of novel compact broadband planar filters," *IEEE Trans. Microw. Theory Tech.*, vol. 51, no. 2, pp. 364–369, Feb. 2003.
- [8] L. Zhu, S. Sun, and W. Menzel, "Ultra-wideband (UWB) bandpass filters using multiple-mode resonator," *IEEE Microw. Wireless Compon. Lett.*, vol. 15, no. 11, pp. 796–798, Nov. 2005.
- [9] L. Zhu, H. Bu, and K. Wu, "Aperture compensation technique for innovative design of ultra-broadband microstrip bandpass filter," in *IEEE MTT-S Int. Microw. Symp. Dig.*, 2000, pp. 315–318.
- [10] J. T. Kuo and E. Shih, "Wideband bandpass filter design with three-line microstrip structures," in *IEEE MTT-S Int. Microw. Symp. Dig.*, 2001, pp. 1593–1596.
- [11] R. W. Jackson and D. W. Matolak, "Surface-to-surface transition via electromagnetic coupling of coplanar waveguide," *IEEE Trans. Microw. Theory Tech.*, vol. MTT-35, no. 11, pp. 1027–1032, Nov. 1987.
- [12] J. J. Burke and R. W. Jackson, "Surface-to-surface transition via electromagnetic coupling of microstrip and coplanar waveguide," *IEEE Trans. Microw. Theory Tech.*, vol. 37, no. 3, pp. 519–525, Mar. 1989.
- [13] L. Zhu and W. Menzel, "Broad-band microstrip-to-CPW transition via frequency-dependent electromagnetic coupling," *IEEE Trans. Microw. Theory Tech.*, vol. 52, no. 5, pp. 1517–1522, May 2004.
- [14] H. Wang, L. Zhu, and W. Menzel, "Ultra-wideband bandpass filters with hybrid microstrip/CPW structure," *IEEE Microw. Wireless Compon. Lett.*, vol. 15, no. 12, pp. 844–846, Dec. 2005.
- [15] K. Li, D. Kurita, and T. Matsui, "An ultra-wideband bandpass filter using broadside-coupled microstrip-coplanar waveguide structure," in *IEEE MTT-S Int. Microw. Symp. Dig.*, 2005, pp. 675–678.
- [16] D. M. Pozar, *Microwave Engineering*, 2nd ed. New York: Wiley, 1998, ch. 8.



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